

# **RHR801**

# Rad-hard very high-speed comparator

Datasheet - production data



## **Features**

- Propagation time of 7 ns
- Rise/fall time: 1.1 ns on 10 pF
- Low consumption: 1.4 mA
- Single supply: 3 V to 5 V
- 100 krad high-dose rate
- SEL-free up to 120 MeV.cm<sup>2</sup>/mg
- SET characterized

## **Applications**

- High-speed timing
- High-speed sampling
- Clock recovery
- Clock distribution
- Phase detectors

## **Description**

The RHR801 is a very high-speed single comparator. It is designed to allow very high rise and fall times while drawing a high noise supply rejection. It uses a high-speed complementary BiCMOS process to achieve its very good speed/power ratio and its high tolerance to radiation. The RHR801 is mounted in a hermetic Flat-8 package.



### **Table 1: Device summary**

### **Notes:**

<span id="page-0-1"></span><span id="page-0-0"></span>(1)SMD: standard microcircuit drawing  $(2)$ EPPL = ESA preferred part list

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This is information on a product in full production. *www.st.com*

## **Contents**





# **1 Absolute maximum ratings and operating conditions**

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#### **Table 2: Absolute maximum ratings**

#### **Notes:**

<span id="page-2-1"></span> $<sup>(1)</sup>$ Vcc is defined as the voltage between the Vcc+ and Vcc- pins. The comparator can be used in single supply</sup> (for example,  $Vcc+ = 5$  V,  $Vcc- = 0$  V) or dual supply (for example,  $Vcc+ = 2.5$  V,  $Vcc- = -2.5$  V).

<span id="page-2-2"></span> $<sup>(2)</sup>$ Differential voltages are the non-inverting input terminal with respect to the inverting input terminal. Vid</sup> should not exceed ±2 V. Diodes should be placed externally between the inputs should this voltage be beyond this range

<span id="page-2-3"></span>(3) If the input voltage goes beyond the rails (above Vcc+ or below Vcc-), the ESD diodes may be activated. It is required in that case to limit the input current to 10 mA with a serial resistor connected on the input.

<span id="page-2-4"></span>(4)Short-circuits can cause excessive heating and destructive dissipation. Values are typical.

<span id="page-2-5"></span> $(5)$ Human body model: a 100 pF capacitor is charged to the specified voltage, then discharged through a 1.5 kΩ resistor between two pins of the device. This is done for all couples of connected pin combinations while the other pins are floating.

<span id="page-2-6"></span>(6)Machine model: a 200 pF capacitor is charged to the specified voltage, then discharged directly between two pins of the device with no external series resistor (internal resistor  $<$  5 Ω). This is done for all couples of connected pin combinations while the other pins are floating.

<span id="page-2-7"></span> $(7)$ Charged device model: all pins and the package are charged together to the specified voltage and then discharged directly to ground through only one pin. This is done for all pins.



#### **Table 3: Operating conditions**



# <span id="page-3-1"></span><span id="page-3-0"></span>**2 Electrical characteristics**

**Table 4: VCC+ = 3.3 V, VCC- = 0 V (unless otherwise specified)**

<b>Symbol</b>	<b>Parameter</b>	<b>Test conditions</b>	Temp.	Min.	Typ.	Max.	<b>Unit</b>
Input characteristics (see Figure 35)							
Vio	Input offset voltage	$V_{ICM} = V_{CC}/2$	$125^{\circ}$ C	$-8.0$		8.0	mV
			$25^{\circ}$ C	$-7.0$	$-0.2$	7.0	
			$-55^{\circ}$ C	$-8.0$		8.0	
VTRIP+	High input threshold	$V_{ICM} = V_{CC}/2$	$125^{\circ}$ C	$-8.0$		8.0	
			$25^{\circ}$ C	$-7.0$	1.1	7.0	
			$-55^{\circ}$ C	$-8.0$		8.0	
VTRIP-	Low input threshold	$V_{ICM} = V_{CC}/2$	$125^{\circ}$ C	$-8.0$		8.0	
			$25^{\circ}$ C	$-7.0$	$-1.5$	7.0	
			$-55^{\circ}$ C	$-8.0$		8.0	
<b>VHYST</b>	Hysteresis	$V_{ICM} = V_{CC}/2$	$25^{\circ}$ C	1.5	2.5	4.0	
Iв	Input bias current	$V_{ICM} = V_{CC}/2$	125°C	$-4$	$-2.2$	0.0	μA
			$25^{\circ}$ C	-5	$-2.5$	0.0	
			$-55^{\circ}$ C	$-7$	$-3.5$	0.0	
$C_{IN}$	Input capacitance		$25^{\circ}$ C		5		pF
Dynamic performances (see Figure 36, Figure 37, and Figure 38)							
TPLH	Logic "0" to logic "1" propagation time	150 mV step, $C_L = 10$ pF, 50 mV overdrive, V <sub>ICM</sub> = Vcc/2	125°C	7.0	8.8	12.0	ns
			$25^{\circ}$ C	6.0	8.1	9.5	
			$-55^{\circ}$ C	6.0	8.1	9.5	
		200 mV step, $C_L = 10$ pF, 100 mV overdrive, $V_{ICM}$ = Vcc/2	125°C	6.5	8.0	10.5	
			$25^{\circ}$ C	5.5	7.8	9.0	
			$-55^{\circ}$ C	5.5	7.8	9.0	
TPHL	Logic "1" to logic "0" propagation time	150 mV step, $C_L = 10$ pF, 50 mV overdrive, V <sub>ICM</sub> = Vcc/2	$125^{\circ}$ C	7.0	9.0	12.0	
			$25^{\circ}$ C	6.0	8.3	9.5	
			$-55^{\circ}$ C	6.0	8.3	9.5	
		200 mV step, $C_L = 10$ pF, 100 mV overdrive, V <sub>ICM</sub> = Vcc/2	$125^{\circ}$ C	6.5	7.9	10.5	
			$25^{\circ}$ C	$5.5$	7.7	9.0	
			$-55^{\circ}$ C	5.5	7.7	9.0	
TR	Output rise time 20 % to 80 %	200 mV step, C <sub>L</sub> = 10 pF	$25^{\circ}$ C		1.4		
$T_F$	Output fall time 80 % to 20 %	200 mV step, $C_L = 10$ pF	$25^{\circ}$ C		1.4		ns
$F_{MAX}$	Maximum input frequency	$V_{in}$ = 1 $V_{P-P}$ sine wave, $C_L = 10$ pF, output duty cycle between 45 % and 55 %	$125^{\circ}$ C	60	74		MHz
			$25^{\circ}$ C	55	72		
			$-55^{\circ}$ C	50	68		
0							





## **Table 5: VCC+ = 5 V, VCC- = 0 V (unless otherwise specified)**

<span id="page-4-0"></span>





**RHR801 Electrical** characteristics





# <span id="page-7-0"></span>**3 Electrical characteristic curves**









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3.0 3.5 4.0 4.5 5.0  $V_{CC}(V)$ 

3.0 3.5 4.0 4.5 5.0  $V_{CC}(V)$ 

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# <span id="page-13-0"></span>**4 Radiations**

## **4.1 Introduction**

<span id="page-13-3"></span><span id="page-13-1"></span>*[Table 6](#page-13-3)* summarizes the radiation performance of the RHF310.



#### **Notes:**

<span id="page-13-4"></span> $<sup>(1)</sup>$ Using the comparator beyond the maximum operating voltage (5 V) may result in significant overconsumption following low-</sup> dose rate radiation at 5.5 V (30 krad at 36 rad/h) and could lead to functional interrupt above 30 krad at 36 rad/h

# **4.2 Total ionizing dose (TID)**

<span id="page-13-2"></span>The products guaranteed in radiation within the RHA QML-V system fully comply with the MIL-STD-883 TM 1019 specification.

The RHR801 is RHA QML-V tested and characterized in full compliance with the MIL-STD-883 specification, both below 10 mrad/s and between 50 and 300 rad/s.

These parameters are shown in *[Table 7](#page-13-5)* and *[Table 8](#page-14-0)* (high-dose rate) and *[Table 9](#page-15-0)* and *[Table 10](#page-16-0)* (low-dose rate), as follows:

- All test are performed in accordance with MIL-PRF-38535 and test method 1019 of MIL-STD-883 for total ionizing dose (TID).
- The initial characterization is performed in qualification only on both biased and unbiased parts, on a sample of ten units from two different wafer lots.
- <span id="page-13-5"></span>• Each wafer lot is tested at both high and low dose rates, in the worst bias case condition, based on the results obtained during the initial qualification.



#### **RHR801 Radiations**



**Table 7: Drift after 300 krad and after annealing, during 24 h @ 25 °C and 168 h at 100 °C, 180 krad/h high-dose rate, VCC+ = 3.3 V, VCC- = 0 V, T = 25 °C, (unless otherwise specified)**

<span id="page-14-0"></span>

### **Radiations RHR801**

<span id="page-15-0"></span>

**Table 8: Drift after 300 krad and after annealing, during 24 h @ 25 °C and 168 h at 100 °C, 180 krad/h high-dose rate, VCC+ = 5 V, VCC- = 0 V, T = 25 °C, (unless otherwise specified)**





**Table 9: Drift after 30 krad, 36 rad/h low-dose rate, VCC+ = 3.3 V, VCC- = 0 V, T = 25 °C, (unless otherwise specified)**

<span id="page-16-0"></span>

### **Radiations RHR801**



**Table 10: Drift after 30 krad, 36 rad/h low-dose rate, VCC+ = 5 V, VCC- = 0 V, T = 25 °C, (unless otherwise specified)**

# **4.3 Heavy ions**

<span id="page-17-0"></span>

The heavy ion trials are performed on qualification lots only. No additional test is performed.



# <span id="page-18-0"></span>**5 Parameters and implementation**

# **5.1 Static input features**

<span id="page-18-3"></span><span id="page-18-1"></span>

# **5.2 Dynamic characteristics**

<span id="page-18-4"></span><span id="page-18-2"></span>



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<span id="page-19-0"></span>

<span id="page-19-1"></span>

**Figure 38: Propagation time**



## **5.3 Characteristics of the output stage**

<span id="page-20-0"></span>The RHR801 uses a rail-to-rail MOS output. The output levels are guaranteed through testing (see the output characteristics in *[Table 4](#page-3-1)* and *[Table 5](#page-4-0)*). This stage is optimized for driving a load of 1 kΩ, with no stability issues. The capacitive load affects both the rise and fall times.

## **5.4 Impedance matching for dynamic measurements**

<span id="page-20-1"></span>To correctly evaluate this high-speed comparator, both the input and output must be properly matched (50 Ω). This matching is mandatory to avoid reflections on the tracks and cables, particularly at such high-speed rise and fall times. The matching of the input is relatively easy to perform with a 50  $\Omega$  input resistance placed as close as possible to the comparator input. The input track is 50  $\Omega$  matched. For the output, the comparator cannot drive a 50 Ω line directly. So, to reduce the output current while keeping a good 50  $\Omega$ termination on both sides of the cable, it is mandatory to use a series resistor much greater than 50 Ω, for example, 1 kΩ as in *[Figure 39](#page-20-3)*.

<span id="page-20-3"></span>



## **5.5 Implementation on the board**

<span id="page-20-2"></span>The RHR801 is a very high-speed product that features very sharp output rise and fall times. The very high current variations must be appropriately managed and proper board layout techniques should be used to ensure best performances.

It is important to minimize the resistance from the source to the input of the comparator. High resistance values combined with the equivalent input capacitance can result in time constants below the capability of the comparator. This is the cause of a lagged response at the input, resulting in an output delay. Moreover, proper ground impedance and other layout techniques must be implemented to minimize the input stray capacitance, such as very short tracks on any high-impedance termination.

With high-speed applications, it is very important to provide bypass capacitors for the power supply. Good power supply decoupling is mandatory (pin 4 and pin 7), as well as good decoupling on the reference (pin 2). With dual supplies, a 10 µF bypass capacitor should be placed on each power supply pin. This capacitor reduces any potential voltage ripple from the power supply at lower frequencies. A 10 nF ceramic capacitor should be placed as close as possible to the power supply pins and be tracked to ground. This capacitor reduces higher frequency noise during high-frequency switching.

A proper ground plane is particularly recommended for high-speed performance. It can be created by implementing a continuous conductive plane all over the surface of the circuit board, with breaks for the necessary paths only. A proper ground plane minimizes the effects of stray capacitance on the circuit board and facilitates the layout of matched tracks.



This ground plane also provides a low inductive ground, eliminating any potential differences at various ground points.









#### **Figure 42: Input impedance matching**



Time constant  $t = R \times Cs$  is should be as low as possible and  $t \ll Tr$ , Tf, Tplh, and Tphl.

## **Figure 43: 50 Ω matching**



Time constant  $t = 50 \Omega \times Cs$  is should be as low as possible and  $t \ll Tr$ , Tf, Tplh, and Tphl.



## **5.6 Application examples**

## **5.6.1 Inverting comparator with hysteresis**

<span id="page-23-1"></span><span id="page-23-0"></span>The RHR801 comparator has a typical 2.5 mV implemented input voltage hysteresis which improves device stability and ensures a clean output response when the input signal amplude is relative small or moving slowly. However, in certain situations, like in noisy environments, it is desirable to increase the hysteresis value. This can easily be done by an external positive feedback network connected to the device.

<span id="page-23-3"></span>

*[Figure 44](#page-23-3)* shows the circuit with positive feedback between the output and non-inverting input. Threshold voltages are given by the R1, R2, and R3 ratio and the V $cc$  power supply voltage. Neglecting input bias current and output voltage drop,  $V_{TH+}$ , and  $V_{TH}$  can be calculated using *[Equation 1](#page-23-4)*.

### <span id="page-23-4"></span>**Equation 1**

$$
V_{TH} = V_{CC} \cdot \frac{R_2}{R_2 + R_1|R_3}
$$

$$
V_{TH} = V_{CC} \cdot \frac{R_2|R_3}{R_1 + R_2|R_3}
$$

The symbol "|" represents a resistors parallel combination. The threshold voltages of *[Figure](#page-23-3)  [44](#page-23-3)* are set to  $V_{TH+}$  = 1.1 V and  $V_{TH-}$  = 1.3 V.

## **5.6.2 Fast signal recovery**

<span id="page-23-2"></span>The circuit in *[Figure 45](#page-24-1)* represents an example of a simple translator input signal from a 50 Ω transmission line to a CMOS compatible output.



<span id="page-24-1"></span>

The reference voltage is set by the resistors  $R_2$  and  $R_3$  to 1.65 V. Capacitor (C) in parallel with  $R_1$  ensure stable low impedance of the reference input during a transition period. A 100-nF capacitor, with low ESR, must be placed close to the device pin.  $C_1$  removes the DC component from the input signal while  $R_1$  terminates the 50  $\Omega$  input and avoids signal reflection. The minimum operating frequency is given by  $C_1$  and it is about 100 kHz.

## **5.6.3 10 MHz RC oscillator**

<span id="page-24-0"></span>The circuit in *[Figure 46](#page-24-2)* provides a square signal with a frequency of about 10 MHz. This circuit utilizes both positive and negative feedback. Positive feedback produces the  $R_2$ ,  $R_3$ , and R4 resistor network which implements input voltage hysteresis described in *[Section](#page-23-1)*  [5.6.1](#page-23-1). Because  $R_2 = R_3 = R_4$ , the threshold voltages are 1/3 of the V<sub>cc</sub> and 2/3 of the V<sub>cc</sub>. Consequently, output duty cycle is 50  $%$  and output frequency is independent of Vcc.

<span id="page-24-2"></span>

The R1 feedback resistor periodically charges and discharges the  $C_1$  capacitor. The output signal period can be calculated using *[Equation 2](#page-25-0)*. Note that this equation is valid only when  $R_2 = R_3 = R_4$ .



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<span id="page-25-0"></span>**Equation 2**

$$
T = \ln(4) \cdot \tau = 1.39 \cdot R_1 \cdot C_1
$$

In a real application, output frequency is slightly lower than calculated due to PCB parasitic capacitances.



# **6 Package information**

<span id="page-26-0"></span>In order to meet environmental requirements, ST offers these devices in different grades of ECOPACK® packages, depending on their level of environmental compliance. ECOPACK® specifications, grade definitions and product status are available at: *www.st.com*. ECOPACK<sup>®</sup> is an ST trademark.



# **6.1 Ceramic Flat-8 package information**

<span id="page-27-0"></span>

The upper metallic lid is not electrically connected to any pins, nor to the IC die inside the package. Connecting unused pins or metal lid to ground or to the power supply will not affect the electrical characteristics.



#### **Table 11: Ceramic Flat-8 mechanical data**





# <span id="page-28-0"></span>**7 Ordering information**



#### **Notes:**

<span id="page-28-1"></span>(1)Specific marking only. Complete marking includes the following: SMD pin (on QML-V flight only) ST logo Date code (date the package was sealed) in YYWWA (year, week, and lot index of week) QML logo (Q or V) Country of origin (FR = France)



Contact your ST sales office for information regarding the specific conditions for products in die form and QML-Q versions.



# <span id="page-29-0"></span>**8 Other information**

## **8.1 Date code**

<span id="page-29-1"></span>The date code is structured as shown below:

- EM xyywwz
- QML-V yywwz

where:

- − x (EM only) = 3 and the assembly location is Rennes, France
- − yy = last two digits of the year
- − ww = week digits
- <span id="page-29-2"></span>− z = lot index in the week

## **8.2 Documentation**

### **Table 13: Documentation provided for each type of product**



### **Notes:**

<span id="page-29-3"></span> $(1)$ QCI = quality conformance inspection

<span id="page-29-4"></span> $(2)$ PIND = particle impact noise detection

<span id="page-29-5"></span> $^{(3)}$ SEM = scanning electron microscope

<span id="page-29-6"></span>(4)List of components that failed during screening





# **9 Revision history**

<span id="page-30-0"></span>

## **Table 14: Document revision history**



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